

Switch Mode Secondary Side Post Regulator

FEATURES

- Precision Secondary Side Post Regulation for Multiple Output Power Supplies
- Useful for Both Single Ended and Center Tapped Secondary Circuits
- Ideal Replacement for Complex Magnetic Amplifier Regulated Circuits
- Leading Edge Modulation
- Does Not Require Gate Drive Transformer
- High Frequency (>500kHz) Operation
- Applicable for Wide Range of Output Voltages
- High Current Gate Driver (0.5A Sink/1.5A Source)
- Average Current Limiting Loop

DESCRIPTION

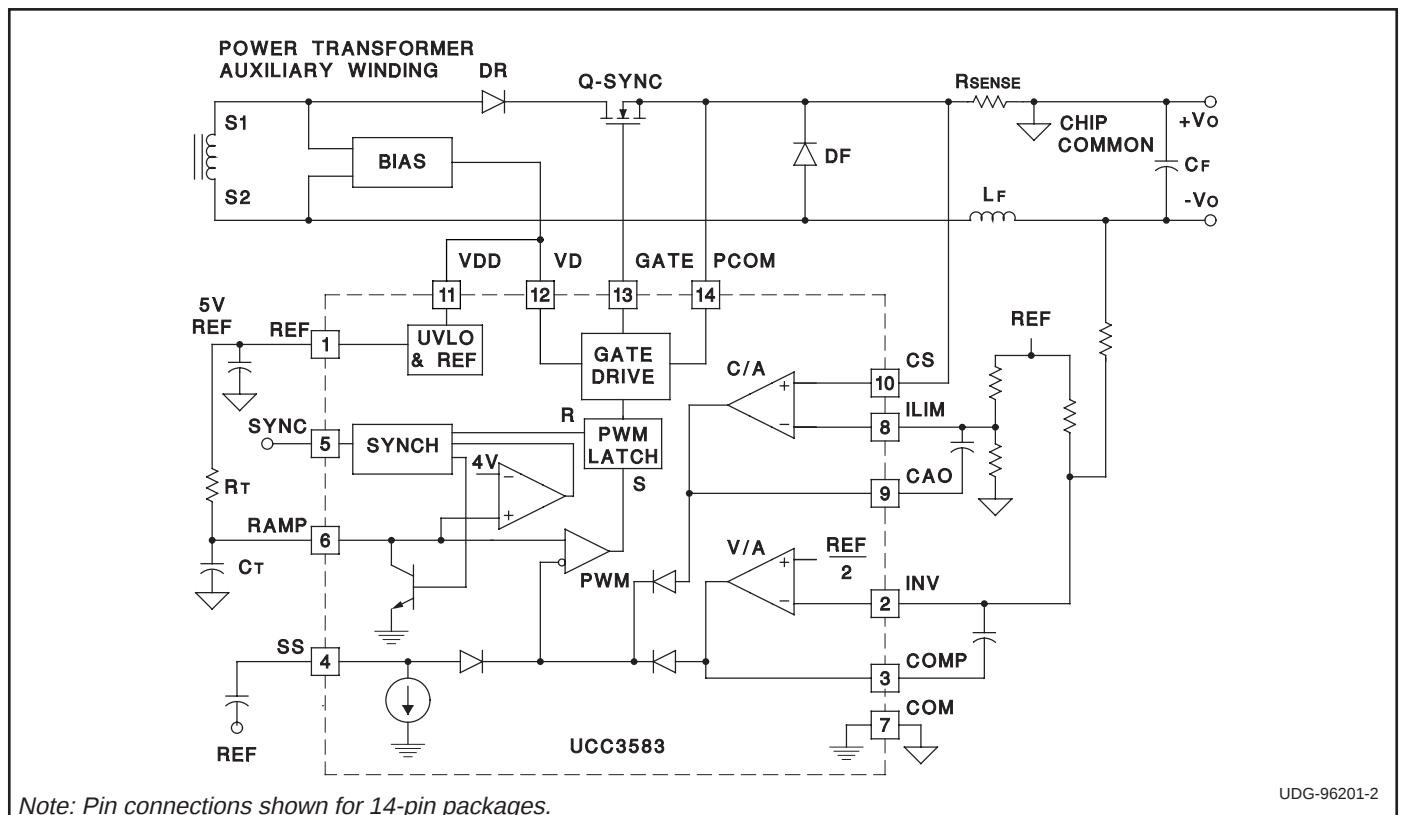
The UCC3583 is a synchronizable secondary side post regulator for precision regulation of the auxiliary outputs of multiple output power supplies. It contains a leading edge pulse width modulator, which generates the gate drive signal for a FET power switch connected in series with the rectifying diode. The turn-on of the power switch is delayed from the leading edge of the secondary power pulse to regulate the output voltage. The UCC3583 contains a ramp generator slaved to the secondary power pulse, a voltage error amplifier, a current error amplifier, a PWM comparator and associated logic, a gate driver, a precision reference, and protection circuitry.

The ramp discharge and termination of the gate drive signal are triggered by the synchronization pulse, typically derived from the falling edge of the transformer secondary voltage. The ramp starts charging again once its low threshold is reached. The gate drive signal is turned on when the ramp voltage exceeds the control voltage. This leading edge modulation technique prevents instability when the UCC3583 is used in peak current mode primary controlled systems.

The controller operates from a floating power supply referenced to the output voltage being controlled. It features an undervoltage lockout (UVLO) circuit, a soft start circuit, and an averaging current limit amplifier. The current limit can be programmed to be proportional to the output voltage, thus achieving foldback operation to minimize the dissipation under short circuit conditions.

(continued)

TYPICAL APPLICATION AND BLOCK DIAGRAM



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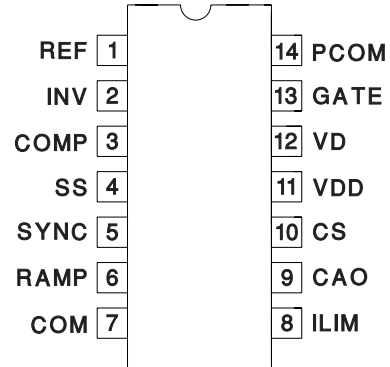
ABSOLUTE MAXIMUM RATINGS

V _{DD}	15V
I _{VDD}	15mA
RAMP	−0.3V to V _{DD} + 1V
I _{RAMP}	5mA
I _{REF}	−30mA
PCOM	−0.2V to 0.2V
I _{GATE} (t _{wp} < 1μs and Duty Cycle < 10%)	−0.8A to 1.8A
I _{COMP}	−5mA to 5mA
I _{CAO}	−5mA to 5mA
V _{SYNC}	−0.6V to V _{REF} + 0.3V
I _{SYNC}	−05mA to 5mA
INV, SS, ILIM, ISENSE	−0.3V to V _{REF} + 0.3V
Storage Temperature	−65°C to +150°C
Junction Temperature	−55°C to +150°C
Lead Temperature (Soldering, 10 sec.)	+300°C

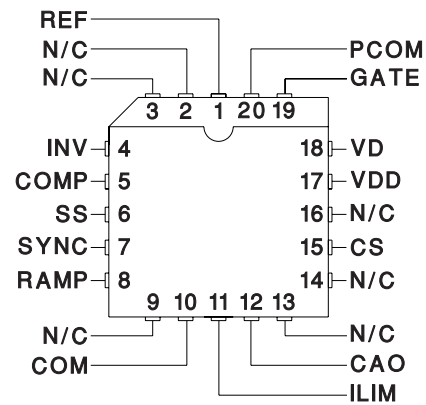
All voltages are with respect to the COM terminal unless otherwise stated. Currents are positive into, negative out of the specified terminal. Consult Packaging Section of Databook for thermal limitations and considerations of packages.

CONNECTION DIAGRAMS

DIL-14, SOIC-14 (Top View)
J, N, or D Packages



PLCC-20 (Top View)
Q Package



ELECTRICAL CHARACTERISTICS: Unless otherwise stated, these specifications apply for T_A = −55°C to 125°C for UCC1583, −40°C to 85°C for UCC2583, and 0°C to 70°C for UCC3583; V_{DD} = 12V, R_T = 60k, C_T = 200pF, T_A = T_J.

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNITS
Ramp Generation and Synchronization					
Maximum Input Operating Frequency	For input with 5% to 90% duty cycle (Note 1)	500			kHz
Ramp Frequency, Free Running		95	100	105	kHz
Ramp Discharge Current	V _{RAMP} = 0.5V	2.0	3.6		mA
Low Threshold Voltage	No min, no max, 0=TYP		0		V
High Threshold Voltage		3.75	4	4.25	V
Synchronizing Threshold Voltage (On)	(Note 1)		1		V
Synchronizing Comparator Hysteresis			1		V
Output Duty Cycle					
Minimum Duty Cycle	Output D/C = Output PW / Input PW			0	%
Maximum Duty Cycle	Output D/C = Output PW / Input PW	100			%

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PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNITS
Voltage Error Amplifier					
V_{INV}	$V_{COMP} = V_{INV}$, 0°C to 70°C (UCC3583)	2.462	2.5	2.538	V
	$V_{COMP} = V_{INV}$, All Other Temperature Ranges	2.45	2.5	2.55	V
I_{INV}	$V_{COMP} = V_{INV}$		300	500	nA
V_{COMP} Low	$V_{INV} = 2.6\text{V}$, $I_{COMP} = 100\mu\text{A}$		450	700	mV
V_{COMP} High	$V_{INV} = 2.4\text{V}$, $I_{COMP} = -100\mu\text{A}$	5.0	5.5	6.0	V
AVOL	No Load	70	90		dB
GBW Product	At $f = 100\text{kHz}$, $T_A = 25^{\circ}\text{C}$ (Note 1)	3	5		MHz
Current Error Amplifier					
Input Offset Voltage				10	mV
Input CM Low	Common Mode for CS and ILIM (Note 1)			0	V
Input CM High	Common Mode for CS and ILIM (Note 1)	2			V
V_{CAO} Low	$V_{+IN} = 0\text{V}$, $V_{-IN} = 0.1\text{V}$, $I_{CAO} = 100\mu\text{A}$		250	500	mV
V_{CAO} High	$V_{+IN} = 0\text{V}$, $V_{-IN} = 0.1\text{V}$, $I_{CAO} = -100\mu\text{A}$	5.0	5.5	6.0	V
Input Current (ILIM and CS Pins)		-50	0	50	nA
AVOL	No Load	70	90		dB
GBW Product	At $f = 100\text{kHz}$, $T_A = 25^{\circ}\text{C}$	2	4		MHz
Soft Start Current			10	25	μA
UVLO					
VDD On Threshold Voltage		8.5	9.0	9.5	V
VDD Off Threshold Voltage		7.9	8.4	8.9	V
UVLO Hysteresis		0.3	0.6	0.9	V
Bias Supply					
Supply Clamp Voltage		13	14	15	V
Supply Current (VDD)	$f = 100\text{kHz}$ With No Gate Output Load		3	5	mA
Output Driver					
V_{SAT} High	$I_{GATE} = -150\text{mA}$		0.6	1.0	V
V_{SAT} Low	$I_{GATE} = 50\text{mA}$		0.4	0.75	V
Rise Time	$C_{GATE} = 1\text{nF}$		50	75	ns
Fall Time	$C_{GATE} = 330\text{pF}$		20	40	ns
Reference					
V_{REF}	$I_{REF} = 0$, 0°C to 70°C (UCC3583)	4.925	5	5.075	V
	$I_{REF} = 0$, All Other Temperature Ranges	4.900	5	5.100	V
Line Regulation	$V_{DD} = 10\text{V}$ to 14V		2	30	mV
Load Regulation	$I_{REF} = 0\text{mA}$ to 2mA		1	20	mV

Note 1: Guaranteed by design. Not 100% tested in production.

PIN DESCRIPTIONS

CAO: Output of the current error amplifier. Averaging of the sensed current signal is provided by connecting an integrating capacitor between ILIM and CAO. CAO feeds into the PWM comparator input and controls the loop when its voltage is higher than the voltage at COMP (output of the voltage error amplifier).

COM: Signal ground for the chip. It is connected to the positive terminal of the output voltage being regulated by the IC.

COMP: Output of the voltage error amplifier fed into the PWM comparator. Loop compensation components are connected between COMP and INV.

CS: Non-inverting input of the current error amplifier. The sensed current signal from the current sense resistor is connected to this pin. By making the signal at CS proportional to the output voltage, effective current foldback limiting can be provided.

GATE: Gate drive output for the power switch FET. The drive pin has a 0.5A sink/1.5A source capability and very low output off-state impedance.

ILIM: Inverting input of the current error amplifier. It sets the DC limit for the output current.

INV: Inverting input of the voltage error amplifier. The feedback signal is connected to this pin using a resistive divider between REF and $-V_o$.

PCOM: Power ground for the chip. It is connected to the source terminal of the MOSFET being regulated by the IC.

RAMP: This pin is the input to the PWM comparator and provides a ramp signal for generation of the PWM signal. A capacitor to COM and a resistor to REF set the charging rate for the ramp. An internal current source of

1mA discharges RAMP when synchronization signal appears or when RAMP crosses a 4V threshold. In the intended mode of operation, the switching frequency is determined by the secondary power pulse. The RC components at RAMP should be selected to give an appropriately sized ramp signal. In the absence of a synchronizing pulse, these RC components determine the free running frequency of the controller.

REF: Precision 5V reference pin. REF stays off until VDD exceeds 9V and turns off again when VDD drops below 8.4V. Bypass REF to COM.

SS: This pin provides a soft start function. A capacitor to REF programs the soft start time. During soft start, the PWM comparator is controlled by the soft start voltage resulting in a slow increase in output duty cycle. Once the soft start capacitor is discharged, output control is dictated by the larger of the output at CAO or COMP.

SYNC: Synchronization input pin. It is connected to a signal representative of the secondary power pulse. One possible implementation is to use a resistive divider between terminal S2 of the secondary winding shown in Figure 1 and REF for generating the input to the SYNC pin. The synchronizing comparator is referenced to 0.5V and has $\pm 500\text{mV}$ of hysteresis. The trip levels are approximate 1.0V and 0.0V. The designer should prevent the SYNC pin from exceeding 0.3V below ground as this will turn on the ESD diode.

VD: Power supply for the output driver. VD should be tied to VDD in the application.

VDD: Power supply for the chip. VDD should be bypassed to COM. VDD has to be 9V for the IC to start and 8.4V for it to remain operational. A shunt clamp from VDD to COM limits the supply voltage to 14V.

APPLICATION INFORMATION

Power Stage Circuit Configuration

The UCC3583 is designed for use in a post regulator application for tightly regulating auxiliary outputs in a multiple output converter. The post regulation is applied to the secondary side power pulse of a power transformer where the power pulse is controlled by the feedback signal from the main output. In order to simplify the application of the UCC3583, it is required that the IC be referenced to the positive output terminal and the output filter inductor be placed in the return path. The placement of the inductor in the return path facilitates better EMI performance, in addition to making magnetic de-

signs and terminations easier to implement. Typical setup and circuit waveforms of the UCC3583 system application are shown in Figure 1. Figure 2 shows waveforms for a single ended output rectifier application of the UCC3583 shown on page 1. The UCC3583 can also be used in half bridge rectifier applications as shown by the circuit and waveforms depicted in Figures 3 and 4. Referencing the IC to the positive output terminal creates a requirement for a floating bias voltage for the IC which can be referenced to the same positive voltage terminal. Possible implementations of deriving the floating bias voltage are shown in Figure 5.

APPLICATION INFORMATION (cont.)

For the circuit shown in Figure 5a, CC1 is charged when the transformer voltage is positive and the synchronous switch is on. During the off period of Q-SYNC, the charge is transferred to CC2 through diode DC2. Diode DC3 charges CC2 during the blocking interval of Q-SYNC. This method is preferable when the transformer positive voltage is high enough to generate the required bias voltage. For the circuit shown in Figure 5b, CC1 is charged during the period when reverse (reset) voltage appears across the secondary. The charge on CC1 is transferred to CC2 through DC2 when Q-SYNC turns on. This method is preferable when the reverse voltage is high enough to generate the required bias voltage. The series resistor should be chosen to handle the required voltage drop at full IC operating current when the zener clamp across VDD and COM is activated.

The following is a description of the major functional blocks of the UCC3583. Refer to Figure 6 (Typical Application Circuit) for component designations.

UVLO and Start Up

The UCC3583 has an internal undervoltage lockout circuit which keeps the internal circuitry inactive until VDD exceeds the upper threshold (9V). Once the chip is activated, VDD has to be above the lower UVLO threshold (8.4V) for it to remain functional. The IC requires a low startup current of only 100μA when VDD is under the UVLO threshold. VDD has an internal clamp of 14V which can sink up to 10mA. Measures must be taken not to exceed this current. The internal reference (REF) is brought up when the UVLO on threshold is exceeded.

The soft start pin provides an effective means to start the IC in a controlled manner. An internal current of 10μA starts discharging a capacitor connected to SS when the UVLO conditions have been removed. The voltage on SS controls the duty cycle of the output during the discharge period.

Synchronizing Circuit and Oscillator

UCC3583 is primarily intended for synchronizable operation where its switching frequency is determined by the secondary pulse of the power transformer. However, it has an internal oscillator which allows it to operate in free-running mode when an external synchronization pulse is not available. The switching frequency is determined by resistor R_T connected between REF and RAMP and capacitor C_T connected from RAMP to GND. The frequency is given by:

$$freq = \frac{1}{t_{CH} + t_{DIS}} \text{ where } t_{CH} = 1.56 \cdot R_T \cdot C_T$$

and

$$t_{DIS} = \frac{C_T \cdot V_{RAMP(p-p)}}{I_{RAMP(dis)}} \approx 3000 \cdot C_T$$

The values of R_T and C_T are also dictated by the fact that the ramp is discharged through an internal impedance of 2k. The value of R_T needs to be at least 50k to ensure that the internal discharge current is the current through R_T during the entire discharge period. This results in making the value of C_T relatively small for a desired frequency of operation.

When the synchronizing signal is available, the oscillator frequency should be programmed to be lower than the synchronizing frequency to ensure proper operation. A large difference in self-running and synchronizing frequencies leads to smaller ramp amplitude and higher noise sensitivity. The ramp capacitor is discharged when the synchronization signal arrives and begins charging when the low threshold is crossed.

There are two methods to synchronize to the secondary pulse. One method is to use the rising edge of the secondary pulse, which reduces the maximum duty cycle available. Subsequently, the post regulator switch cannot be turned on during the C_T discharge time. The other method is to use the falling edge of the secondary pulse for synchronization. This method is preferable because it allows a slower discharge of the ramp capacitor without affecting the maximum available duty cycle of the post regulator. The UCC3583 SYNC input needs to reach a fixed threshold (1.0V typical) for synchronization to take effect. Hence the IC is usable with either method of synchronization. However, the UCC3583 oscillator configuration is better suited for synchronization to the falling edge. A recommended method to implement the synchronization is shown in Figure 6. By connecting SYNC to a resistive divider between REF and the secondary terminal S2, the synchronization is achieved whenever the voltage on S2 goes from a negative value to zero. R_A and R_B should be selected so that the voltage on the SYNC pin varies from 0V to 1V. Placement of a Schottky diode from SYNC to COM prevents the voltage at SYNC from going negative. The internal hysteretic SYNC comparator has an inverting input set to 0.5V with about ±0.5V hysteresis.

PWM Comparator

The UCC3583 uses a leading edge PWM scheme. In a leading edge PWM, the output pulse (gate signal) is turned on when the error amplifier crosses the PWM ramp and turned off by the clock/oscillator. Leading edge modulation is naturally provided by magamp type post regulators and is an essential feature for post regulators. Without the leading edge modulation in a multiple output

APPLICATION INFORMATION (cont.)

converter with post regulation on one or more outputs, the primary current shape does not remain monotonic and can lead to instability when the primary current is used for current mode control or current limiting. When compared to conventional trailing edge PWMs, the leading edge modulation leads to a phase inversion that needs to be accounted for in the feedback loop. For the UCC3583, this inversion is automatically provided since the sensed voltage at the power supply output negative terminal has a negative polarity with respect to the chip common. Thus, UCC3583 does not require inverting buffers which would otherwise be needed.

Error Signal Generation and Current Limiting

The PWM comparator in the UCC3583 is controlled by three parallel loops with only one of them in effect at a time. During normal operation, the voltage error amplifier output is fed to the PWM comparator. The voltage error amplifier can be compensated using commonly used feedback techniques to achieve the desired dynamic performance. The output drive capability of the voltage amplifier is limited to 100 μ A, so appropriately high impedances should be used to utilize the full output swing of the amplifier. During startup, the soft start ca-

pacitor controls the pulse width. The third control loop is provided by the average current amplifier. By sensing the instantaneous inductor current and filtering/averaging it with the current error amplifier, accurate current limiting is achieved. This loop is in effect only during the overcurrent mode and provides a more accurate and noise free control of the maximum output current compared to conventional peak current limiting circuits. The current limit is set by programming the voltage at ILIM based on the current sense resistor chosen. In addition, the current limit can be made proportional to the output voltage in order to limit the power dissipation under short circuit conditions. This is implemented by inserting a bias voltage on CS which is proportional to the output voltage.

Gate Drive Circuit

The gate drive circuit of the UCC3583 provides high current drive capability and is very easy to implement as a result of tying the chip common to the source of the switching device. Turn on current is higher (1.5A) as fast turn on is essential for low losses and effective operation. During the turn off, the drain voltage disappears, so turn off time can be slower without increasing switching losses.

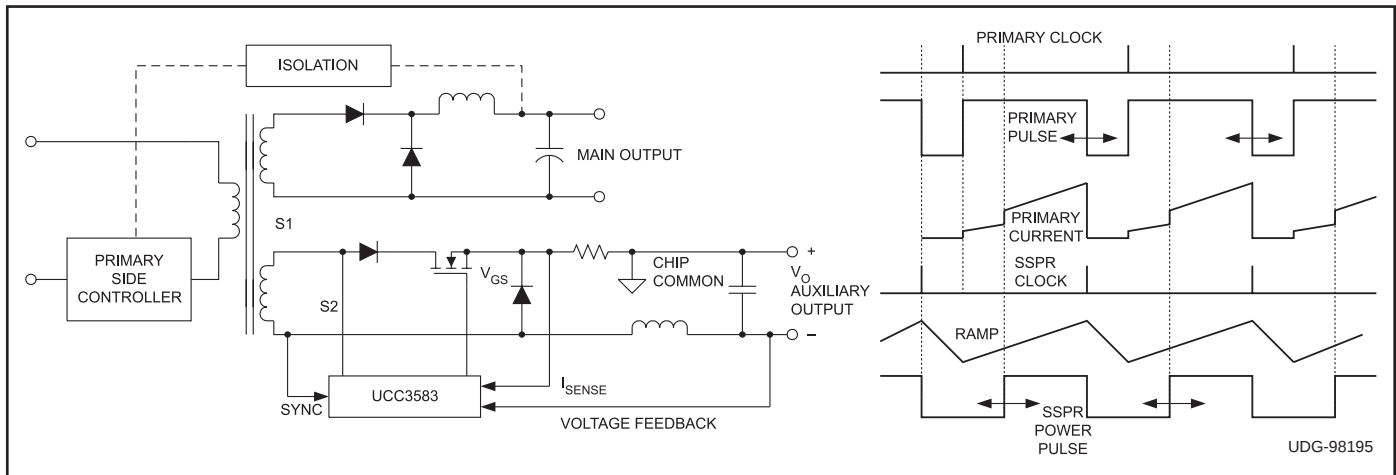


Figure 1. UCC3583 SSPR system application and typical waveforms.

APPLICATION INFORMATION (cont.)

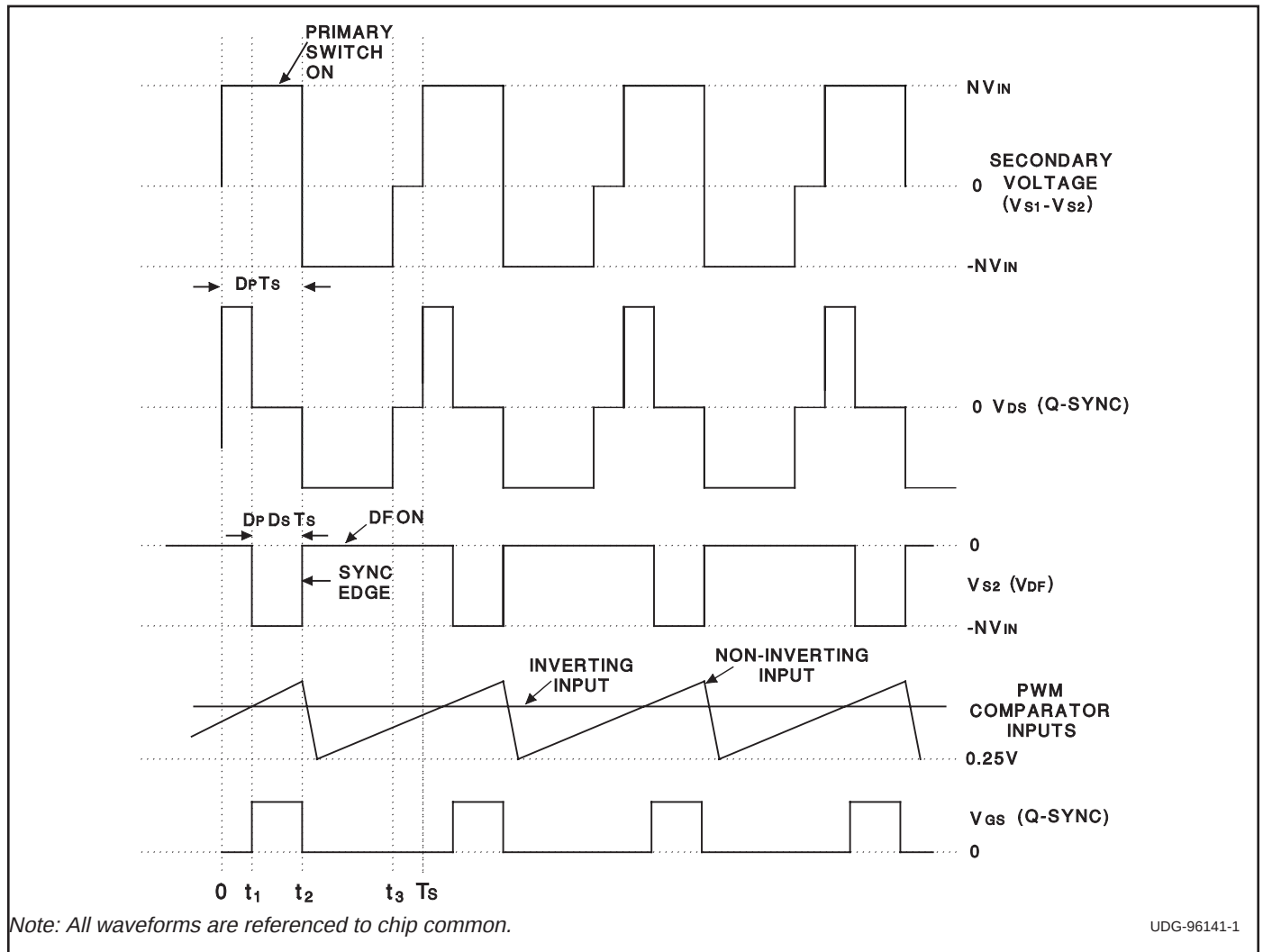


Figure 2. Single ended post regulator waveforms.

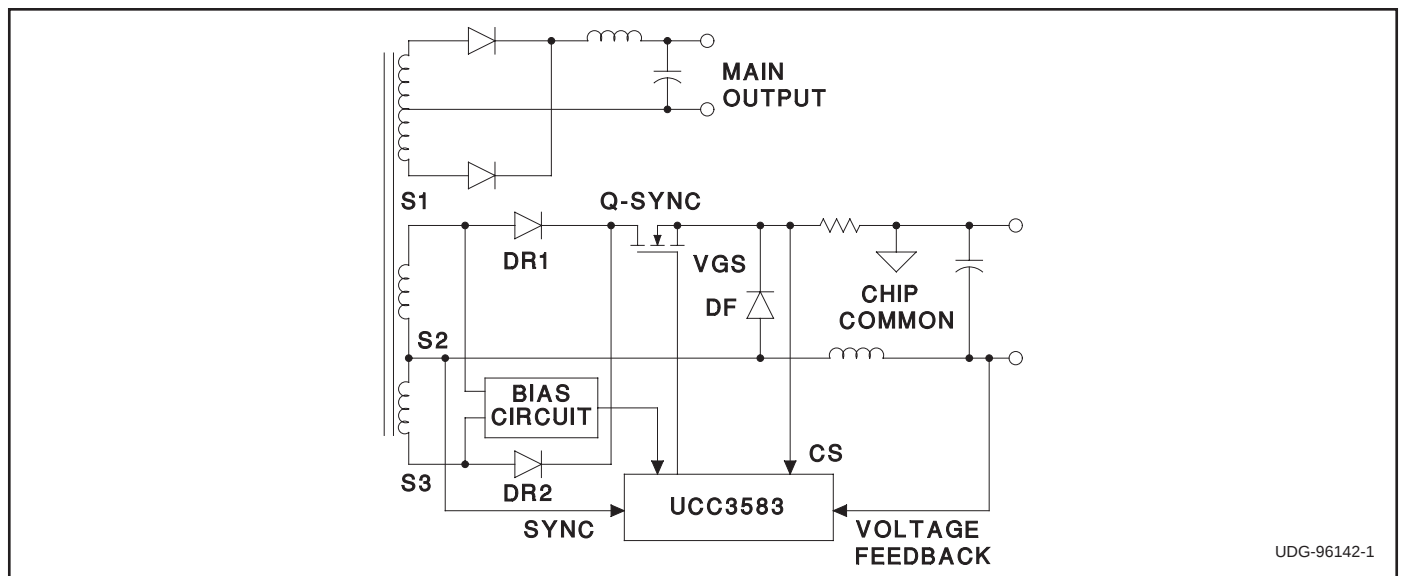


Figure 3. Half-bridge synchronous post regulator application.

APPLICATION INFORMATION (cont.)

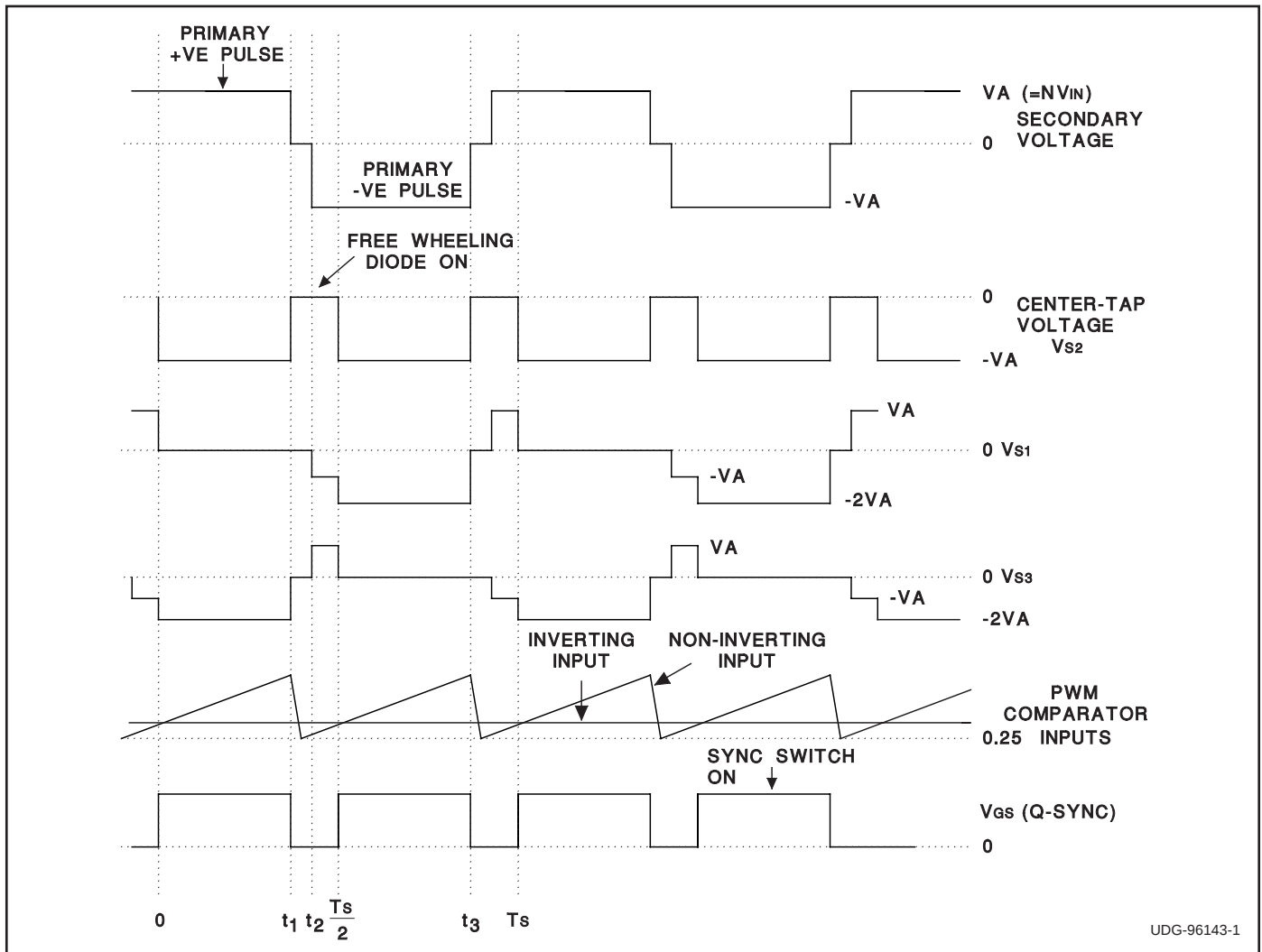


Figure 4. Half-bridge synchronous post regulator to waveforms.



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Figure 5. Possible implementation for floating bias voltage generation.



Figure 6. Typical application circuit.

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